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(54) Title: HIGH RESOLUTION PHASE FREQUENCY DETECTORS

High Resolution Extension of the HRPD Config.2
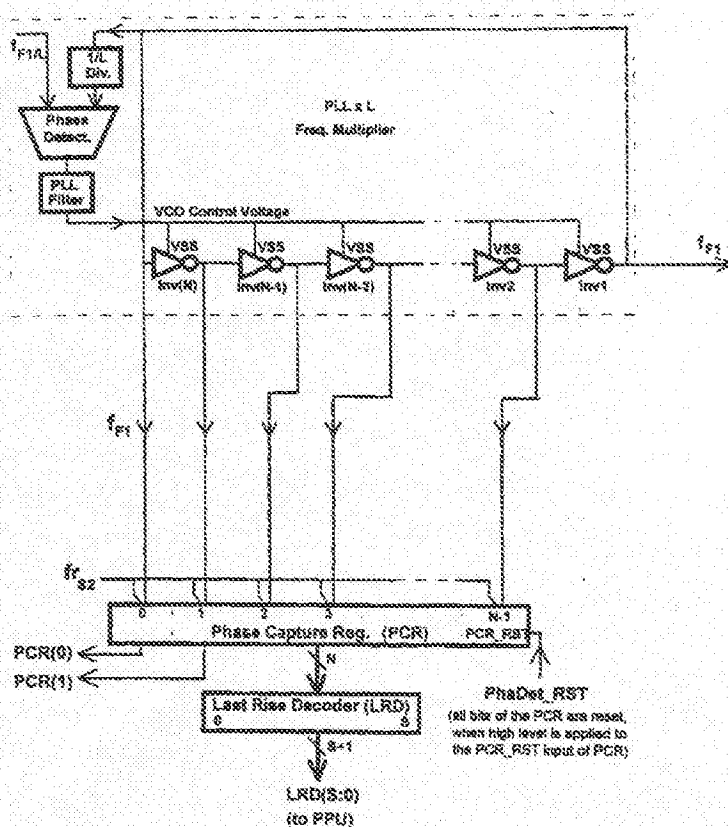
(57) Abstract: A digital phase detector comprises a frame measurement configuration for counting a first signal clock during every frame of a second signal and for buffering the counted value until it is read by a phase processing unit. In particular this invention allows using size limited clock counters for measurements of unlimited time ranges by combining unlimited number of intermediate samples without accumulating samples granularity errors. In addition to the measurements of the final time ranges, the intermediate samples are available for purposes of digital signal processing.

WO 01/91297 A3

(54) Title: HIGH RESOLUTION PHASE FREQUENCY DETECTORS

(57) Abstract: An inexpensive and reliable, high resolution digital phase detector for timing circuits for wireless, optical or wireline transmission systems. In particular this invention allows using size limited clock counters for measurements of unlimited time ranges by combining unlimited number of intermediate samples without accumulating samples granularity errors. In addition to the measurements of the final time ranges, the intermediate samples are available for purposes of digital signal processing.

High Resolution Phase Frequency Detectors

BACKGROUND OF THE INVENTION

1. Field of the invention

This invention is directed to providing high resolution low cost digital phase detectors
which can be used in digital phase locked loops (DPLLs) and shall also make possible
other replacements of analog circuits by their digital implementations.
The high resolution phase detectors (HRPD) can be used for a wide range of data
rates, and for wireless, optical , or wireline transmission and communication systems.

2. Background art

Most of currently used digital phase detectors have resolution limited by a clock cycle
time.
While some most advanced digital phase detectors allow higher resolutions which are
comparable with propagation delays of clock propagating gates, they have other
limitations such as: complex algorithms which are conditioned by propagation delays
of detector timing circuits, and dependency of their phase resolution on technological
process and power supply variations.

There is a need for digital phase detectors which have simpler algorithms and greater
independence versus the propagation delays of the detector timing circuits and the
clock propagating gates.

SUMMARY OF THE INVENTION

1. Purpose of the invention

It is an object of present invention to provide digital high resolution phase detectors
which are simple and reliable and can be used in variety of communication systems.

2. General description of the invention

Variety of the high resolution phase detectors are described in this document using the
same terms which are explained below.
First signal clock f_o is a higher frequency signal which is used to measure time periods
corresponding to single or multiple cycles of a lower frequency signal which is called
second signal frame fr_{sz}.

High resolution phase detectors comprise:
- a counter and a buffer configuration for counting the first signal clock during every
   frame of a second signal, and for buffering the counted value until it is read by a
   phase processing unit;
- a high resolution extension of the counter and buffer configuration, which measures a
   remainder of a frame phase skew which is lesser than one clock cycle;
- a detector timing circuit for synchronizing the clock counting and the buffer reading
   versus the signal frame related phase capture into a phase capture register;
- a high resolution phase processing method for combining contents of the clock
   counter and the phase capture register into a high resolution phase measurement.

The high resolution extension can be implemented by using a propagation circuit and a
phase capture register, as it is explained below.
The first signal clock or the measured second signal frame is propagated through
multiple serially connected gates.
The first signal clock or the second signal frame is captured in the phase capture
register by the outputs of the serially connected gates, or the outputs of the serially
connected gates are captured in the phase capture register by the first signal clock or
by the second signal frame.
The content of the phase capture register is used to calculate a phase skew of the
second signal frame versus the first signal clock.

The high resolution phase processing method comprises:
- a calculation of an approximate phase error between the first signal and the second
   signal, by subtracting a number of first signal clock cycles which corresponds to zero
   phase skew of the second signal frame, from a last number of clock cycles which has
   been read from the buffer;
- a calculation of a high resolution phase error by adding the high resolution extension
   to the approximate phase error;
- elimination of phase error accumulations for multiple measurements, by subtracting
   last high resolution extension from a period of the first signal clock, and by adding
   the resulting remainder of the clock cycle to an adjacent phase error measurement.

The above design principles and methods allow designing multiple different
implementations of HRPD.
Some of these HRPD implementations are defined below and are shown with more
details in the section DESCRIPTION OF THE PREFERRED EMBODIMENTS.

3. HRPD Config.1 based on delay line captured by frame edge

The HRPD Config.1 uses:
- an open ended delay line which is built with multiple serially connected gates, which
   the first signal clock is continuously propagated through;
- a leading edge of the second signal frame to capture a status of the outputs of the

delay line in the phase capture register;
- a calibration method of gates propagation delays, which is based on capturing the
  whole cycle of the first signal clock as it is propagated along the delay line and
  dividing the first signal cycle time by the number of gates which carried the whole
  cycle propagation.

The calibration method comprises:
- statistical averaging of the calibration result, in order to eliminate most of a
  granularity error caused by capturing of the integer gates number and to reduce an
  error caused by power supply ripple.

The calibration method can further comprise a reduction of an error caused by an
occurrence of different gate delays at the end versus the front of the delay line:
- by assigning higher weights to the cycle gate number, if captured cycle propagating
  gates are located at the front of the delay line;
- by using the weighted cycle gate numbers for the statistical averaging of the
  calibration result.

4. HRPD Config.2 based on ring oscillator captured by frame edge.

The HRPD Config.2 uses:
- the signal propagation circuit which is built with multiple serially connected gates
  forming a ring oscillator which is phase locked to the first signal clock;
- a leading edge of the second signal frame to capture a status of the outputs of the ring
  oscillator gates in the phase capture register.
Since the number of ring oscillator gates and the first signal clock period are known,
calibration of gates propagation delay is not needed for the HRPD Config.2.

5. HRPD Config.3 based on clock signal captured by frame delay line edges.

The HRPD Config.3 uses:
- the signal propagation circuit which is built with multiple serially connected gates
  forming an open ended delay line, which the second signal frame is continuously
  propagated through;
- the outputs of the delay line gates to capture a waveform of the first signal clock, in
  the phase capture register;
- a calibration method of gates propagation delays, which is based on capturing the
  whole cycle of the first signal clock as it occurs along the inputs of the phase capture
  register, and dividing the first signal cycle time by the number of the delay line
  gates which outputs captured the whole clock cycle.

The calibration method comprises:
- statistical averaging of the calibration result, in order to eliminate most of a
  granularity error caused by having an integer number of the capturing gates, and to
  reduce an error caused by power supply ripples.

The calibration method can further comprise a reduction of an error caused by an occurrence of different gate delays at the end versus the front of the delay line:
- by assigning higher weights for the cycle capturing gate number, if the cycle capturing gates are located at the front of the delay line;
- by using the weighted cycle gate numbers for the statistical averaging of the calibration result.

6. HRPD Config.4 based on frame delay line captured by clock signal.

The HRPD Config.4 uses:
- the signal propagation circuit which is built with multiple serially connected gates forming an open ended delay line, which the second signal frame is continuously propagated through;
- the outputs of the delay line gates are captured by rising edges of the first signal clock in phase capture registers;
- a calibration method of gates propagation delays which is based on capturing the frame delay line by 2 consecutive first signal rises, and dividing the first signal cycle time by a difference between numbers of gate delays which were captured by the consecutive first signal rises.

The calibration method comprises:
- statistical averaging of the calibration result, in order to eliminate most of a granularity error caused by capturing an integer number of the delay line gates, and to reduce an error caused by power supply ripples.

The calibration method can further comprise a reduction of an error caused by an occurrence of different gate delays at the end versus the front of the delay line:
- by assigning higher weights to the cycle capturing gate number, if the cycle capturing gates are located at the front of the delay line;
- by using the weighted cycle gate numbers for the statistical averaging of the calibration result

7 HRPD Config.5 based on frame captured by clock delay line.

The HRPD Config.5 uses:
- the signal propagation circuit which is built with multiple serially connected gates forming an open ended delay line, which the first signal clock is continuously propagated through;
- the outputs of the delay line gates to capture a rise of the second signal frame in the phase capture register;
- a calibration method of gates propagation delays which is based on:
  - capturing a frame rising edge by two consecutive rising edges of the signal clock which occur simultaneously along the delay line;
  - and dividing the first signal cycle time by a number of delay line gates which

existed between said clock edges when they captured simultaneously the frame
rising edge in the capture register;
- a capture synchronization method which prevents the next propagated clock edges
from overwriting said captures of the frame rise by said two consecutive clock edges.

The calibration method comprises:
- statistical averaging of the calibration result, in order to eliminate most of a
granularity error caused by having an integer number of the capturing gates, and to
reduce an error caused by power supply ripples.

The calibration method can further comprise a reduction of an error caused by an
occurrence of different gate delays at the end versus the front of the delay line:
- by assigning higher weights to the cycle capturing gate number, if the cycle capturing
gates are located at the front of the delay line.
- by using the weighted cycle gate numbers for the statistical averaging of the
calibration result

8. HRPD Config.6 based on frame captured by ring oscillator.

The HRPD Config.6 uses:
- outputs of the signal propagation circuit, which is built with multiple serially
connected gates forming a ring oscillator which is phase locked to the first signal
clock;
- the outputs of the ring oscillator gates to capture a rise of the second signal frame in
the phase capture register;
- a capture synchronization method which prevents next propagated clock edges from
overwriting said capture of the rise of the second signal frame.

Since the number of ring oscillator gates and the first signal clock period are known,
calibration of gates propagation delay is not needed for the HRPD Config.6.

DESCRIPTION OF THE PREFERRED EMBODIMENTS

1. HRPD Config.1 based on delay line captured by frame edge

The HRPD Config.1 is shown in Fig.1.

Approximate phase measurements are explained below.
The HRPD Config.1 uses two symmetrical phase counters buffers A/B (PCBA/PCBB),
which perform reverse functions during alternative A/B cycles of the frame signal fr_{s2}.
During the A cycle, the PCBA counts the number of incoming f_{s1} clocks, but during the
following B cycle the PCBA remains frozen until its content is read by a phase
processing unit (PPU), and subsequently the PCBA is reset before the beginning of the

next A cycle. Reversibly, the PCBB performs counting during the B cycle and is read and reset during the following A cycle.

Such symmetrical PCBA/PCBB configuration allows much more time for counters propagation by inhibiting counting long before the actual reading takes place. Therefore, much higher frequencies of counted clocks are allowed for the same IC technology.

Generally speaking the above concept of a digital phase detector, represents one of several possible HRPD solutions, which are based on counting the first signal clock during every frame of the second signal, wherein the second signal frame contains a number of the second signal clocks.

The symmetrical twin pair PCBA/PCBB configuration:
- allows higher counting speeds by eliminating all problems related to counters propagation delays.
- allows measurements of fr_{s1} versus f_{p1} phase errors, with a resolution of a single f_{p1} period.

When fr_{s2} rise signals the end of the current phase measurement, counting of f_{p1} clock is inhibited and the counter content remains frozen, until the next rise of the fr_{s2} signal when the counted clock is enabled again. The whole fr_{s2} cycle is a very long freeze period, which is more than sufficient to accommodate; any kind of counter propagation, the counter transfer to the phase processing unit, and the counter reset. During the freeze period a mate counter is kept enabled and provides measurement of fr_{s2} phase.

More detailed operations of the PCBA/PCBB configuration for both alternatives STOPA=1 and STOPB=1, are further explained below.
When STOPA signal is active, HRPD circuits perform listed below functions.
The PCBB counts all rising edges of f_{p1} clocks.
When PCBB(9) goes high, the PCBB generates SEL9 signal. The SEL9 activates RD_REQ which initiates the PPU to read PCBA via CNTR(15:0).
The PPU calculates an approximate phase error of previous fr_{s2} versus f_{p1}, by subtracting from the newly read PCB, the number N of f_{p1} clocks which nominally should correspond to the frame fr_{s2}.
When CTRB(14) goes high, the PCBB generates SEL14 signal. The SEL14 activates RST_PCBA which initiates PCBA reset circuits after its content has been read by PPU.
When fr_{s2} rise occurs, PRESTOP_FF is set to 1 and inverts STOPA/STOPB signals.
When STOPB signal is active all the above functionality is fulfilled with reversed roles of STOPB and PCBA versus STOPA and PCBB.

High resolution extension of phase measurements is explained below.
The high resolution extension enhances phase detection resolution to a single inverter delay i.e. by ~10times compared with conventional methods based on clock counting.
The high resolution measurement is implemented in the HRPD Config.1, by using the phase capture register (PCR) to measure a positioning of the last rising edge of the second signal frame fr_{s2} versus the f_{p1} clock waveform
The phase capture register captures a state of outputs of multiple serially connected

gates which the first signal clock f_{p1} is continuously propagated through, at the leading edge of the second signal frame fr_{s2}.

PCR decoders are used in the high resolution extension, and they are defined below.

The last rise decoder (LRD) provides binary encoded position of f_{p1} rising edge, which has been captured at the most right location of the PCR.

The cycle length decoder (CLD) provides binary encoded lengths of the f_{p1} wave, which has been captured between these 2 falling or 2 rising edges of the f_{p1} wave which occurred at the most right locations of the PCR.

Captured PCR content is decoded by the last rise decoder and the cycle lengths decoder. Contents of the LRD and the CLD are later transferred to the phase processing unit (PPU).

The above operations are controlled by a Detector Timing Circuit, which is shown in the Fig.1.

Timing analysis of the detector timing circuit is shown in Fig.2 and is explained below.

The High Clock Region Flip-Flop (HCR_FF) is set to 1, when f_{p1} rise encounters PCR(0) set to 1. The PCR(0) was set to 1, if an fr_{s2} rise encountered f_{p1}=high. Therefore the HCR_FF=1 signals, that fr_{s2} rising edge occurred during the f_{p1}=high halfcycle.

The PCR(1) is set to 1, when an fr_{s2} rise encounters f_{p1} = low. Therefore the PCR(1)=1 signals, that fr_{s2} rising edge occurred during the f_{p1}=low halfcycle.

PRESTOP_FF is set to 1, when f_{p1} fall encounters HCR_FF or PCR(1) set to 1.

STOP_FF is reversed, by any rising edge of the PRESTOP_FF. Any STOP_FF switching causes a reversal of the PCBA/PCBB functions.

The whole PCR is reset by the signal PhaDet_RST. The PhaDet_RST shall be generated during fr_{s2}=low halfcycle and after contents of the PCR decoders are read by the phase processing unit.

It shall be noticed that a first f_{p1} rise which occurs after fr_{s2} rise, will encounter unchanged status of the STOP_FF. Therefore presently active counter will be increased by 1 by the first f_{p1} rise, but it will be freezed when following f_{p1} fall will reverse the STOP_FF before an arrival of the second f_{p1} rise.

However since STOP_FF reversal was similarly delayed during previous fr_{s2} measurement, presently active counter missed counting one f_{p1} rise at the beginning of the present measurement.

Therefore the counter content needs to be decreased by 1, in order to represent a correct number of complete f_{p1} cycles which occurred between consecutive rising edges of the fr_{s2} frame.

Phase processing method combines the approximate phase measurement and the high resolution extension into an actual phase measurement of a frame signal.

The phase processing method uses additional terms which are explained below.

Calculated by PPU, measured phase (MEA_PHA) represents the actual phase error between fr_{s2} versus the equivalent f_{p1} frame; and consists of the listed below

components.

LRD/CLD is a normalized value of a phase error between fr_{s2} rise versus last f_{ri} rise, as it has been read by the PPU from the LRD and CLD decoders.

Remaining phase error (REM_PHA) is calculated based on the present measurement results, but PPU stores and uses it to correct the next measurement result. The REM_PHA represents a remainder of a presently captured fraction of the f_{ri} period, which needs to be added to the next phase error measurement.

Subtracted N which is a nominal number of first signal clocks per a second signal frame: transforms the counted number of f_{ri} cycles per fr_{s2} period, into an approximate phase error between the fr_{s2} versus the f_{ri}.

While the LRD/CLD represents a normalized PCR captured extension of the CNTR(15:0) captured phase, and is added to the present MEA_PHA: the remaining phase error between the fr_{s2} and the next f_{ri} rise amounts to (CLD-LRD)/CLD and it is stored as the REM_PHA, in order to modify next measurement's MEA_PHA.

Therefore:

$$MEA\_PHA = REM\_PHA + CNTR - 1 + LRD/CLD - N,$$
$$REM\_PHA = (CLD - LRD)/CLD.$$

2. HRPD Config.2 based on ring oscillator captured by frame edge

For the approximate phase measurements the HRPD Config.2 uses the same circuits as the HRPD Config.1.

High resolution extension for the Config.2 has differences versus the Config.1, which are shown in the Fig.3 and are listed below:
- instead of using the open ended delay line as a first clock signal propagation circuit, the ring oscillator which generates f_{ri} clock in the PLLxL Freq. Multiplier is used as said propagation circuit;
- the cycle lengths decoder CLD is eliminated, because a number of active gates in the ring oscillator is known.

The phase capture register captures the state of outputs of multiple serially connected gates which form the ring oscillator which the first signal clock f_{ri} is continuously propagated through, at the leading edge of the second signal frame fr_{s2}.

Since the ring oscillator gates must use lowered power supply, in order to allow their delays controllability in the PLL configuration: phase detection resolution will be slightly lower for the Config.2 versus the Config.1, but it still shall be significantly better when compared with conventional methods limited to clock counting.

The detector timing circuit and the timing analysis are the same for the Config.2 as for the Config.1 (see Fig.1 and Fig.2).

The only difference between a phase processing method of the Config.2 versus the Config.1 is: that since ring gates number (RGN) is always known, the Config.2 does

not need to use the cycle lengths decoder and the CLD can be replaced by a ring gates number (RGN) in the equations calculating the MEA_PHA and the REM_PHA. Therefore:

$$MEA\_PHA = REM\_PHA + CNTR - 1 + LRD/RGN\ -N,$$
$$REM\_PHA = (RGN - LRD)/RGN\ .$$

3. HRPD Config.3 based on clock signal captured by frame delay line edges.

For the approximate phase measurements the HRPD Config.3 uses the same circuits as the HRPD Config.1.
High resolution extension for the Config.3 has differences versus the Config.1, which are shown in the Fig.4 and are listed below:
- instead of propagating the f_{Pi} clock through a delay line, the second signal frame is propagated through the delay line, and outputs of the delay line gates are used to capture the f_{Pi} clock in corresponding bits of the phase capture register (PCR);
- the first rise decoder (FRD) is used in the Config.3 instead of the last rise decoder (LRD) from the Config.1, since the PCR content represents f_{Pi} waveform occurring after a rising edge of the fr_u frame;
- a new bit PCR(-1) is added to the PCR, in order to capture inverted f_{Pi} value which was captured in the PCR(1) bit for the Config.1.
Since non inverting gates must be used in the delay line, resolution is reduced compared with the Config.1, but still is significantly better than with conventional methods.

For the detector timing circuits, the HRPD Config.3 uses similar solutions as the HRPD Config.1: with the exception of using the signal PCR(-1) (see Fig.5), instead of the signal PCR(1) (see Fig.1) to enable activation of the PRESTOP_FF by the first falling edge of the f_{Pi}.
The timing analysis is very similar for the Config.3 (see Fig.6) as for the Config.1 (see Fig.2). The differencies are caused by the fact that for the Config.3 parts of waveforms which occur after the rising edges of the frame signal are captured, and therefore the captured waveforms are shown on the right sides of the arrows indicating appearances of the frame rising edges.

Phase processing method for the Config.3 is explained below.
Since for the Config.3, the PCR and its decoders represent a part of a waveform which occurs after a frame rising edge:
- a content of the FRD divided by the CLD, represents a REM_PHA value which shall be added to the next measurement,
- a fraction of the f_{Pi} cycle which shall be added to the present measurement amounts to: 1-FRD/CLD = (CLD-FRD)/CLD.
Therefore:

$$MEA\_PHA = REM\_PHA + CNTR-1 + (CLD-FRD)/CLD - N,$$
$$REM\_PHA = FRD/CLD.$$

4. HRPD Config.4 based on frame delay line captured by clock signal.

For the approximate phase measurements the HRPD Config.4 uses the same circuits as the HRPD Config.1.

High resolution extension for the Config.4 has differences versus the Config.1, which are shown in the Fig.7 and are explained below.
Instead of propagating the f_{p1} clock through a delay line, the second signal frame is propagated through the delay line, and the outputs of the delay line gates are captured after any rising edge of the second signal frame:
- the first f_{p1} clock captures the frame delay line in the front phase capture register (FPCR);
- the second f_{p1} clock captures the frame delay line in the end phase capture register (EPCR).
A bit FPCR(-1) is used in the FPCR for capturing present value of the second signal frame fr_{s2} by the falling edge of the first signal clock f_{p1}.
The last frame decoder (LFD) provides a binary encoded position of the fr_{s2} rising edge versus the first following f_{p1} rising, which has been captured on the right side of the FPCR.
The cycle length decoder (CLD) provides a binary encoded lengths of the f_{p1} wave which is calculated as a difference between a number of gate delays captured in the EPCR versus a number of gate delays captured in the FPCR.

Detector Timing Circuit for the Config.4 has differences versus the Config.1, which are shown in the Fig.8 and are explained below.
FPCR(-1) is used to activate the HCR_FF which enables activation of the PRESTOP_FF, if an fr_{s2} rise occurred during f_{p1} = high condition.
FPCR(0) is used directly to enable activation of the PRESTOP_FF, if an fr_{s2} rise occurred during f_{p1} = low condition.
An inverted PRESTOP_FF is used as active low STOPFN signal: in order to preserve the frame delay line captured in the FPCR by the first f_{p1} clock after a rising edge of fr_{s2}.
Normally all the rising edges of the f_{p1} clock keep capturing the frame delay line in the FPCR, until the capturing is inhibited by STOPFN = low. Since STOPFN = low is generated between the first and the second f_{p1} rise after the rising edge of fr_{s2}, the final content of the FPCR is the delay line captured by the first f_{p1} rise.
Similarly an active low STOPEN signal is generated between the second and the third f_{p1} rise after the rising edge of fr_{s2}. Since STOPEN = low inhibits further capturing of the frame delay line in the EPCR, the final content of the EPCR is the delay line captured by the second f_{p1} rise.

Timing analysis for the Config.4 is shown in the Fig.9.

The timing diagrams show both capture events: the delay line capturing by the first f_{n} rise, and the delay line capturing by the second f_{n} rise.

The FPCR(-1) is activated before the FPCR(0): if fr_{s2} rise occurs during f_{n} = high condition and is captured by f_{n} fall. Similarly the FPCR(0) is activated before the FPCR(-1): if fr_{s2} rise occurs during f_{n} = low condition and is captured by f_{n} rise.

The STOPFN is shown to be activated as STOPFN = low by the f_{n} fall after the first f_{n} rise. Similarly the STOPEN is shown to be activated as STOPEN = low by the f_{n} fall after the second f_{n} rise.

Phase processing method for the Config.4 is defined below.

LFD/CLD is a normalized value of a phase error between an fr_{s2} rise versus the first f_{n} rise, as it has been read by PPU from the LFD and CLD decoders.

The content of the LFD divided by the CLD, represents a REM_PHA value which shall be added to the next measurement.

A fraction of the f_{n} cycle which shall be added to the present measurement amounts to:
1-LFD/CLD = (CLD-LFD)/CLD.

Therefore:

$$MEA\_PHA = REM\_PHA + CNTR-1 + (CLD-LFD)/CLD - N,$$
$$REM\_PHA = LFD/CLD.$$

5. HRPD Config.5 based on frame captured by clock delay line.

For the approximate phase measurements the HRPD Config.5; uses the same circuits as the HRPD Config.1.

High resolution extension for the Config.5 has differences versus the Config.1, which are shown in Fig.10 and are explained below.

The Config.5 implements said capture synchronization method:
- by using the gates from G0 to GR to prevent the delay line outputs from capturing fr_{s2} = high into any PCR bit whenever the next PCR bit has been set to 1 before;
- by using the delayed phase capture register (DPCR) to provide PCR content which is delayed by f_{n} halfcycle, in order to assure sufficient pulse duration for PCR input clocks.

For some integrated circuit technologies, PCR flip-flops propagation delays may be sufficient to provide said required pulse duration. Therefore for such technologies the DPCR is not needed, since an output of the next PCR bit can be connected directly to an inverter which prevents delay line output from passing through the gate connected to the clock input of the current PCR bit.

The outputs of the delay line gates which the f_{n} clock is propagated through, keep capturing 0s in the PCR for as long as the second signal frame remains low.

When a rising edge of the fr_{s2} appears (see also Fig.12):

- the fr_{s2} rise is captured in the PCR simultaneously by two rising edges of the delay line outputs, which are separated by a number of delay gates which corresponds to f_{r1} cycle;
- the two rising edges keep propagating along the delay line and keep capturing $fr_{s2} =$ high in consecutive PCR bits for as long as encountered PCR bits have proceeding bits not set to 1;
- in addition to said two rising edges, a third rising f_{r1} edge enters the delay line from an f_{r1} source and will keep propagating and capturing $fr_{s2} =$ high until a bit is encountered which is proceeded by a set to 1 bit.

Therefore:
- the first delay line rising edge will set all the bits starting from its fr_{s2} detection bit down to the end of PCR;
- the second delay line rising edge will set all the bits starting from its fr_{s2} detection bit until it encounters the bit which follows the fr_{s2} detection bit of the first line rising edge;
- the third delay line rising edge will set all the bits starting from the delay line entry until it encounters the bit which follows the fr_{s2} detection bit of the second line rising edge.

A bit PCR(-1) is used in the PCR for capturing present value of the second signal frame fr_{s2}, by the falling edge of the first signal clock f_{r1}.

First frame decoder (FFD) provides binary encoded position of the fr_{s2} rising edge versus the last proceeding f_{r1} rising which has been captured on the left side of the PCR as the fr_{s2} detection bit of the second line rising edge.

Cycle length decoder (CLD) provides binary encoded lengths of the f_{r1} wave, which is calculated as a number of gate delays between: the fr_{s2} detection bit of the first line rising edge, and the fr_{s2} detection bit of the second line rising edge.

Since non inverting gates must be used in the delay line, the resolution is reduced compared with the Config.1, but still is significantly better than with conventional methods.

Detector Timing Circuit for the Config.5 has differences versus the Config.1, which are shown in the Fig.11 and are explained below.

PCR(-1) is used to activate the HCR_FF which enables PRESTOP_FF activation, if an fr_{s2} rise occurred during f_{r1}=high condition.

PCR(0) directly enables PRESTOP_FF activation, , if an fr_{s2} rise occurred during f_{r1}=low condition.

Phase processing method for the Config.5 is explained below.

FFD/CLD is a normalized value of a phase error between an fr_{s2} rise versus the last f_{r1} rise, as it has been read by the PPU from the FFD and the CLD decoders.

The content of the FFD divided by the CLD shall be added to the present phase

measurement.

A fraction of the f_{ri} cycle which shall be added to the next measurement amounts to:

1-FFD/CLD = (CLD-FFD)/CLD.

Therefore:

MEA_PHA = REM_PHA + CNTR-1 + FFD/CLD - N,

REM_PHA = (CLD-FFD)/CLD.

6. HRPD Config.6 based on frame captured by ring oscillator.

For the approximate phase measurements, the HRPD Config.6 uses the same circuits as the HRPD Config.5.

High resolution extension for the Config.6 has differences versus the Config.5, which are shown in the Fig.13 and Fig.14 and are explained below.

Instead of the open ended delay line, the outputs of the ring oscillator which is phase locked to a stable clock, are used to capture a rise of the fr_{ri} signal in the PCR.

Since the number of ring oscillator gates and the f_{ri} clock period are known, a calibration of the gates propagation delays is not needed for the HRPD Config.6, and the CLD is not needed as well.

Since the calibration is not needed, and the oscillator gates delays cover all the f_{ri} clock period; the PCR can be much shorter, as it needs to cover only one f_{ri} clock period.

The Config.6 uses PLLxL Freq. Multiplier to provide the ring oscillator which is phase locked to a stable reference clock. Therefore ring oscillator gates are the serially connected gates which the f_{ri} is propagated through, and are used to capture a rise of the second signal frame. The ring oscillator gates must use lower power supply in order to allow their delays controllability in the PLL configuration.

Therefore, resolution is slightly reduced compared with the Config.5, but still is significantly better than with conventional methods.

The detector timing circuit is the same for the Config.6 as for the Config.5.

The timing analysis is very similar for the Config.6 as for the Config.5. The only difference is that the PCR content is much shorter, since only one f_{ri} clock period needs to be captured.

The only difference between the phase processing method of the Config.6 versus the Config.5 is: that since ring gates number (RGN) is always known, the Config.6 does not need to use the cycle lengths decoder and the CLD can be replaced by the RGN in the equations calculating the MEA_PHA and the REM_PHA.

Therefore:

MEA_PHA = REM_PHA + CNTR-1 + FFD/RGN - N

REM_PHA = (RGN-FFD)/RGN